NCS199A1R, NCS199A2R, NCS199A3R

Current-Shunt Monitors, Voltage Output, Bidirectional, Zero-Drift, Low- or High-Side Current Sensing

The NCS199A1R, NCS199A2R, and NCS199A3R are voltage output, current shunt monitors (also called current sense amplifiers) which can measure voltage across shunts at common-mode voltages from −0.3 V to 26 V, independent of supply voltage. The low offset of the zero-drift architecture enables current sensing across the shunt with maximum voltage drop as low as 10 mV full-scale. These devices can operate from a single +2.2 V to +26 V power supply, drawing a maximum of 80 μA of supply current, and are specified over the extended operating temperature range (−40°C to +125°C). Available in the SC70–6 package.

Features

• Wide Common Mode Input Range: −0.3 V to 26 V
• Supply Voltage Range: 2.2 V to 26 V
• Low Offset Voltage: ±150 μV max
• Low Offset Drift: 0.5 μV/°C max
• Low Gain Error: 1.5% max
• Low Gain Error Drift: 10 ppm/°C
• Rail-to-Rail Output Capability
• Low Current Consumption: 40 μA typ, 80 μA max

Typical Applications

• Current Sensing (High-Side/Low-Side)
• Telecom
• Power Management
• Battery Charging and Discharging

ORDERING INFORMATION
See detailed ordering, marking and shipping information on page 2 of this data sheet.
NCS199A1R, NCS199A2R, NCS199A3R

ORDERING INFORMATION

<table>
<thead>
<tr>
<th>Device</th>
<th>Gain</th>
<th>R3 and R4</th>
<th>R1 and R2</th>
<th>Marking</th>
<th>Package</th>
<th>Shipping†</th>
</tr>
</thead>
<tbody>
<tr>
<td>NCS199A1RSQT2G</td>
<td>50</td>
<td>20 kΩ</td>
<td>1 MΩ</td>
<td>AZ3</td>
<td>SC70–6</td>
<td>3000 / Tape and Reel</td>
</tr>
<tr>
<td>NCS199A2RSQT2G</td>
<td>100</td>
<td>10 kΩ</td>
<td>1 MΩ</td>
<td>AZ4</td>
<td>SC70–6</td>
<td>3000 / Tape and Reel</td>
</tr>
<tr>
<td>NCS199A3RSQT2G</td>
<td>200</td>
<td>5 kΩ</td>
<td>1 MΩ</td>
<td>AZY</td>
<td>SC70–6</td>
<td>3000 / Tape and Reel</td>
</tr>
</tbody>
</table>

†For information on tape and reel specifications, including part orientation and tape sizes, please refer to our Tape and Reel Packaging Specifications Brochure, BRD8011/D.
Table 1. MAXIMUM RATINGS

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Value</th>
<th>Unit</th>
</tr>
</thead>
<tbody>
<tr>
<td>Supply Voltage (Note 1)</td>
<td>$V_S$</td>
<td>+30</td>
<td>V</td>
</tr>
<tr>
<td>Analog Inputs</td>
<td>$(V_{IN+} - (V_{IN-}))$</td>
<td>−30 to +30</td>
<td>V</td>
</tr>
<tr>
<td>Common–Mode (Note 2)</td>
<td>$(GND-0.3)$ to +30</td>
<td></td>
<td></td>
</tr>
<tr>
<td>REF Input</td>
<td>$V_{REF}$</td>
<td>(GND−0.3) to $(V_s+0.3)$</td>
<td>V</td>
</tr>
<tr>
<td>Output (Note 2)</td>
<td>$V_{OUT}$</td>
<td>(GND−0.3) to $(V_s+0.3)$</td>
<td>V</td>
</tr>
<tr>
<td>Input Current into Any Pin (Note 2)</td>
<td></td>
<td>5</td>
<td>mA</td>
</tr>
<tr>
<td>Maximum Junction Temperature</td>
<td>$T_{J(\text{max})}$</td>
<td>+150</td>
<td>°C</td>
</tr>
<tr>
<td>Storage Temperature Range</td>
<td>$T_{STG}$</td>
<td>−65 to +150</td>
<td>°C</td>
</tr>
<tr>
<td>ESD Capability, Human Body Model (Note 3)</td>
<td>$HBM$</td>
<td>±2000</td>
<td>V</td>
</tr>
<tr>
<td>Charged Device Model (Note 3)</td>
<td>$CDM$</td>
<td>±2000</td>
<td>V</td>
</tr>
<tr>
<td>Latch–Up Current (Note 4)</td>
<td>$I_{LU}$</td>
<td>100</td>
<td>mA</td>
</tr>
</tbody>
</table>

Stresses exceeding those listed in the Maximum Ratings table may damage the device. If any of these limits are exceeded, device functionality should not be assumed, damage may occur and reliability may be affected.

1. Refer to ELECTRICAL CHARACTERISTICS, RECOMMENDED OPERATING RANGES and/or APPLICATION INFORMATION for safe operating parameters.
2. Input voltage at any pin may exceed the voltage shown if current at that pin is limited to 5 mA.
3. This device series incorporates ESD protection and is tested by the following methods:
   - ESD Human Body Model tested per JEDEC standard JS−001−2017.
   - ESD Charged Device Model tested per JEDEC standard JS−002−2014.
4. Latch–up Current tested per JEDEC standard JESD78E.

Table 2. RECOMMENDED OPERATING RANGES

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Min</th>
<th>Typ</th>
<th>Max</th>
<th>Unit</th>
</tr>
</thead>
<tbody>
<tr>
<td>Common–Mode Input Voltage</td>
<td>$V_{CM}$</td>
<td>−0.3</td>
<td>12</td>
<td>26</td>
<td>V</td>
</tr>
<tr>
<td>Supply Voltage</td>
<td>$V_S$</td>
<td>2.2</td>
<td>5</td>
<td>26</td>
<td>V</td>
</tr>
<tr>
<td>Ambient Temperature</td>
<td>$T_A$</td>
<td>−40</td>
<td>125</td>
<td>°C</td>
<td></td>
</tr>
</tbody>
</table>

Functional operation above the stresses listed in the Recommended Operating Ranges is not implied. Extended exposure to stresses beyond the Recommended Operating Ranges limits may affect device reliability.

Table 3. THERMAL CHARACTERISTICS (Note 5)

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Value</th>
<th>Unit</th>
</tr>
</thead>
<tbody>
<tr>
<td>Thermal Resistance, Junction–to–Air (Note 6)</td>
<td>$R_{\text{JJA}}$</td>
<td>250</td>
<td>°C/W</td>
</tr>
</tbody>
</table>

5. Refer to ELECTRICAL CHARACTERISTICS, RECOMMENDED OPERATING RANGES and/or APPLICATION INFORMATION for safe operating parameters.
6. Values based on copper area of 645 mm² (or 1 in²) of 1 oz copper thickness and FR4 PCB substrate.
Table 4. ELECTRICAL CHARACTERISTICS
At $T_A = +25°C$, $V_{SENSE} = V_{IN+} - V_{IN-}$, $V_S = +5$ V, $V_{IN+} = 12$ V, and $V_{REF} = V_S/2$, unless otherwise noted. Boldface limits apply over the specified temperature range of $T_A = -40°C$ to $125°C$, guaranteed by characterization and/or design.

<table>
<thead>
<tr>
<th>Symbol</th>
<th>Parameter</th>
<th>Test Conditions</th>
<th>Min</th>
<th>Typ</th>
<th>Max</th>
<th>Unit</th>
</tr>
</thead>
<tbody>
<tr>
<td>$V_{CM}$</td>
<td>Common–Mode Input Voltage Range</td>
<td>$V_{IN+} = 0$ V to $+26$ V, $V_{SENSE} = 0$ mV, $T_A = -40°C$ to $125°C$</td>
<td>$-0.3$</td>
<td>26</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>CMRR</td>
<td>Common–Mode Rejection Ratio</td>
<td>$V_{SENSE} = 0$ mV</td>
<td>$100$</td>
<td>$120$</td>
<td></td>
<td>dB</td>
</tr>
<tr>
<td>$V_{OS}$</td>
<td>Offset Voltage RTI (Note 7)</td>
<td>$V_{SENSE} = 0$ mV</td>
<td>$\pm 5$</td>
<td>$\pm 150$</td>
<td></td>
<td>$\mu$V</td>
</tr>
<tr>
<td>$dV_{OS}/dT$</td>
<td>RTI vs Temperature (Note 7)</td>
<td>$T_A = -40°C$ to $+125°C$</td>
<td>$0.1$</td>
<td>$0.5$</td>
<td></td>
<td>$\mu$V/$°C$</td>
</tr>
<tr>
<td>PSRR</td>
<td>RTI vs Power Supply Ratio (Note 7)</td>
<td>$V_S = +2.7$ V to $+26$ V, $V_{IN+} = 18$ V, $V_{SENSE} = 0$ mV</td>
<td>$\pm 0.1$</td>
<td>$\pm 10$</td>
<td></td>
<td>$\mu$V/V</td>
</tr>
<tr>
<td>$I_{IB}$</td>
<td>Input Bias Current</td>
<td>$V_{SENSE} = 0$ mV</td>
<td>39</td>
<td>60</td>
<td></td>
<td>$\mu$A</td>
</tr>
<tr>
<td>$I_{IO}$</td>
<td>Input Offset Current</td>
<td>$V_{SENSE} = 0$ mV</td>
<td>$\pm 0.1$</td>
<td></td>
<td></td>
<td>$\mu$A</td>
</tr>
<tr>
<td>$G$</td>
<td>Gain</td>
<td>NCS199A1R</td>
<td>50</td>
<td></td>
<td>V/V</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>NCS199A2R</td>
<td>100</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>NCS199A3R</td>
<td>200</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>$E_G$</td>
<td>Gain Error</td>
<td>$V_{SENSE} = -5$ mV to $5$ mV, $T_A = -40°C$ to $125°C$</td>
<td>$\pm 0.2$</td>
<td>$\pm 1.5$</td>
<td></td>
<td>%</td>
</tr>
<tr>
<td></td>
<td>Gain Error vs Temperature</td>
<td>$T_A = -40°C$ to $125°C$</td>
<td>3</td>
<td>10</td>
<td></td>
<td>ppm/$°C$</td>
</tr>
<tr>
<td></td>
<td>Nonlinearity Error</td>
<td>$V_{SENSE} = -5$ mV to $5$ mV</td>
<td>$\pm 0.01$</td>
<td></td>
<td></td>
<td>%</td>
</tr>
<tr>
<td>$C_L$</td>
<td>Maximum Capacitive Load</td>
<td>No sustained oscillation</td>
<td>1</td>
<td></td>
<td>nF</td>
<td></td>
</tr>
<tr>
<td>$V_{OH}$</td>
<td>Swing to $V_S$ Power Supply Rail</td>
<td>$R_L = 10$ k$\Omega$ to GND, $T_A = -40°C$ to $+125°C$</td>
<td>$V_S - 0.075$</td>
<td>$V_S - 0.2$</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>$V_{OL}$</td>
<td>Swing to GND</td>
<td>$R_L = 10$ k$\Omega$ to GND, $T_A = -40°C$ to $+125°C$</td>
<td>$V_{GND} + 0.005$</td>
<td>$V_{GND} + 0.05$</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>$BW$</td>
<td>Bandwidth ($f_{-3db}$)</td>
<td>NCS199A1R</td>
<td>90</td>
<td></td>
<td>kHz</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>NCS199A2R</td>
<td>60</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>NCS199A3R</td>
<td>40</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>SR</td>
<td>Slew Rate</td>
<td>1</td>
<td></td>
<td>V/$\mu$S</td>
<td></td>
<td></td>
</tr>
<tr>
<td>$e_n$</td>
<td>Voltage Noise Density</td>
<td>$f = 1$ kHz</td>
<td>45</td>
<td></td>
<td>$\mu$V/$\sqrt{Hz}$</td>
<td></td>
</tr>
</tbody>
</table>

7. RTI = referenced–to–input

Product parametric performance is indicated in the Electrical Characteristics for the listed test conditions, unless otherwise noted. Product performance may not be indicated by the Electrical Characteristics if operated under different conditions.
TYPICAL CHARACTERISTICS (T_A = 25°C, V_S = 5 V, V_{IN+} = 12 V and V_{REF} = V_S/2 unless otherwise noted.)

(The NCS199A3R is used for Typical Characteristics)

Figure 1. Input Offset Voltage Production Distribution

Figure 2. Input Offset Voltage vs. Temperature

Figure 3. Common-Mode Rejection Production Distribution

Figure 4. Common-Mode Rejection Ratio vs. Temperature

Figure 5. Gain Error Production Distribution

Figure 6. Gain Error vs. Temperature
TYPICAL CHARACTERISTICS (TA = 25°C, VS = 5 V, VR+ = 12 V and VREF = VS/2 unless otherwise noted.)
(The NCS199A3R is used for Typical Characteristics)

Figure 7. Gain vs. Frequency

Figure 8. Power Supply Rejection Ratio vs. Frequency

Figure 9. Common-Mode Rejection Ratio vs. Frequency

Figure 10. Positive Output Voltage Swing vs. Output Current, VS = 2.2 V

Figure 11. Negative Output Voltage Swing vs. Output Current, VS = 2.2 V

Figure 12. Positive Output Voltage Swing vs. Output Current, VS = 2.7 V
TYPICAL CHARACTERISTICS (TA = 25°C, VS = 5 V, VIN+ = 12 V and VREF = VS/2 unless otherwise noted.)
(The NCS199A3R is used for Typical Characteristics)

**Figure 13.** Negative Output Voltage Swing vs. Output Current, VS = 2.7 V

**Figure 14.** Positive Output Voltage Swing vs. Output Current, VS = 5 V

**Figure 15.** Negative Output Voltage Swing vs. Output Current, VS = 5 V

**Figure 16.** Positive Output Voltage Swing vs. Output Current, VS = 26 V

**Figure 17.** Negative Output Voltage Swing vs. Output Current, VS = 26 V

**Figure 18.** Input Bias Current vs. Common-Mode Voltage with VS = 5 V
TYPICAL CHARACTERISTICS (TA = 25°C, VS = 5 V, VIN+ = 12 V and VREF = VS/2 unless otherwise noted.)
(The NCS199A3R is used for Typical Characteristics)

Figure 19. Input Bias Current vs. Common–Mode Voltage with VS = 0 V (Shutdown)

Figure 20. Input Bias Current vs. Temperature

Figure 21. Quiescent Current vs. Temperature

Figure 22. Voltage Noise Density vs. Frequency

Figure 23. 0.1 Hz to 10 Hz Voltage Noise (Referred to Input)

Figure 24. Step Response (10 mVpp Input Step)
TYPICAL CHARACTERISTICS (TA = 25°C, V_S = 5 V, V_IN+ = 12 V and V_REF = V_S/2 unless otherwise noted.)
(The NCS199A3R is used for Typical Characteristics)

![Common-Mode Voltage Transient Response](image1)

![Inverting Differential Input Overload](image2)

![Noninverting Differential Input Overload](image3)

![Start-Up Response](image4)

![Brownout Recovery](image5)
Current Sensing Techniques

The NCS199AxR current-sense amplifiers can be configured for both low-side and high-side current sensing. Low-side sensing appears to have the advantage of being straightforward, inexpensive, and can be implemented with a simple op amp circuit. However, the NCS199AxR series of devices provides the full differential input necessary to get accurate shunt connections, while also providing a built-in gain network with precision difficult to obtain with external resistors. While at times the application requires low-side sensing, only high-side sensing can detect a short from the positive supply line to ground. Furthermore, high-side sensing avoids adding resistance to the ground path of the load being measured. The sections below focus primarily on high-side current sensing.

Unidirectional Operation

In unidirectional current sensing, the current always flows in the same direction. Common applications for unidirectional operation include power supplies and load current monitoring. Figure 30 shows the NCS199AxR circuit implementation for unidirectional operation using high-side current sensing.

Basic connections for unidirectional operation include connecting the load power supply, connecting a current shunt to the differential inputs of the NCS199AxR, grounding the REF pin, and providing a power supply for the NCS199AxR. The NCS199AxR can be connected to the same power supply that it is monitoring current from, or it can be connected to a separate power supply. If it is necessary to detect short circuit current on the load power supply, which may cause the load power supply to sag to near zero volts, a separate power supply must be used on the NCS199AxR. When using multiple supplies, there are no restrictions on power supply sequencing.

When no current is flowing though the \( R_{\text{SHUNT}} \) and the REF pin is connected to ground, the NCS199AxR output is expected to be within 50 mV of ground. When current is flowing through \( R_{\text{SHUNT}} \), the output will swing positive, up to within 200 mV of the applied supply voltage, \( V_S \).

Bidirectional Operation

In bidirectional current sensing, the current measurements are taken when current is flowing in both directions. For example, in fuel gauging, the current is measured when the battery is being charged or discharged. Bidirectional operation requires the output to swing both positive and negative around a bias voltage applied to the REF pin. The voltage applied to the REF pin depends on the application. However, most often it is biased to either half of the supply voltage or to half the value of the measurement system reference. Figure 31 shows bidirectional operation with three different circuit choices that can be connected to the REF pin to provide a voltage reference to the NCS199AxR.

Figure 30. Basic Unidirectional Connection

Figure 31. Bidirectional Operation

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The REF pin must always be connected to a low impedance circuit, such as in the Figure 31(b), (c), and (d). The REF pin can be connected directly to any voltage supply or voltage reference (shunt or series). However, if a resistor divider network is used to provide the reference voltage, a unity gain buffer circuit must be used, as shown in Figure 31(d).

In bidirectional applications, any voltage that exceeds $V_S + 0.3\, \text{V}$ applied to the REF pin will forward bias an ESD diode between the REF pin and the $V_S$ pin. Note that this exceeds the Absolute Maximum Ratings for the device.

**Input and Output Filtering**

Filtering at the input or output may be required for several different reasons. In this section we will discuss the main considerations with regards to these filter circuits.

In some applications, the current being measured may be inherently noisy. In the case of a noisy signal, filtering after the output of the current sense amplifier is often simpler, especially where the amplifier output is fed into high impedance circuitry. The amplifier output node provides the greatest freedom when selecting components for the filter and is very straightforward to implement, although it may require subsequent buffering.

Other applications may require filtering at the input of the current sense amplifier. Figure 32 shows the recommended schematic for input filtering.
Input filtering is complicated by the fact that the added resistance of the filter resistors and the associated resistance mismatch between them can adversely affect gain, CMRR, and V_{OS}. The effect on V_{OS} is partly due to input bias currents as well. As a result, the value of the input resistors should be limited to 10 kΩ or less. Ideally, select the capacitor to exactly match the time constant of the shunt resistor and its inductance; alternatively, select the capacitor to provide a pole below that point. As an example, a filtering frequency of 100 kHz would require an 82 nF capacitor. The capacitor can have a low voltage rating, but should have good high frequency characteristics.

Make the input filter time constant equal to or larger than the shunt and its inductance time constant:

$$\frac{L_{\text{SHUNT}}}{R_{\text{SHUNT}}} \geq 2 \cdot R_{\text{FILT}} \cdot C_{\text{FILT}}$$

This simplifies to determine the value of $C_{\text{FILT}}$ based on using 10 kΩ resistors for each $R_{\text{FILT}}$:

$$C_{\text{FILT}} \geq \frac{L_{\text{SHUNT}}}{20R_{\text{SHUNT}}}$$

If the main purpose is to filter high frequency noise, the capacitor should be increased to a value that provides the desired filtering.

As the shunt resistors decrease in value, shunt inductance can significantly affect frequency response. At values below 1 mΩ, the shunt inductance causes a zero in the transfer function that often results in corner frequencies in the low 100’s of kHz. This inductance increases the amplitude of high frequency spike transient events on the current sensing line that can overload the front end of any shunt current sensing IC. This problem must be solved by filtering at the input of the amplifier. Note that all current sensing IC’s are vulnerable to this problem, regardless of manufacturer claims. Filtering is required at the input of the device to resolve this problem, even if the spike frequencies are above the rated bandwidth of the device.

Advantages When Used for Low−Side Current Sensing

The NCS199AxR series offer many advantages for low−side current sensing. The true differential input is ideal for connection to either Kelvin Sensing shunts or conventional shunts. Additionally, the true differential input rejects the common−mode noise often present even in low−side current sensing. The NCS199AxR also provides a reference pin to set the output offset from an external reference. Providing all of these features in a tiny package makes the NCS199AxR very competitive when compared to discrete op amp solutions.

Designing for Input Transients Exceeding 30 Volts

For applications that have transient common−mode voltages greater than 30 volts, external input resistors of 10 kΩ provide a convenient location to add either Zener diodes or transient voltage suppression diodes (also known as TVS diodes). There are two possible configurations: one using a single TVS diode with diodes across the amplifier inputs as shown in Figure 33, and the second configuration using two TVS diodes as shown in Figure 34.
Use Zener diodes or unidirectional TVS diodes with clamping voltage ratings up to a maximum of 30 volts. Select TVS diodes with the lowest voltage rating possible for use in the system. There is a wide range between standoff voltage and maximum clamping voltage in TVS diodes. Most diodes rated at a standoff voltage of 18 V have a maximum clamping voltage of 29.2 V. Refer to the TVS data sheet and the parameters of your power supply to make the selection. In general, higher power TVS diodes demonstrate a sharper clamping knee; providing a tighter relationship between rated breakdown and maximum clamping voltage.

Selecting the Shunt Resistor

The desired accuracy of the current measurement determines the precision, shunt size, and the resistor value. The larger the resistor value, the more accurate the measurement possible, but a large resistor value also results in greater current loss.

For the most accurate measurements, use four terminal current sense resistors, as shown in Figure 35. It provides two terminals for the current path in the application circuit, and a second pair for the voltage detection path of the sense amplifier. This technique is also known as Kelvin Sensing. This insures that the voltage measured by the sense amplifier is the actual voltage across the resistor and does not include the small resistance of a combined connection. When using non-Kelvin shunts, follow manufacturer recommendations on how to lay out the sensing traces closely.
NCS199A1R, NCS199A2R, NCS199A3R

Current Output Configuration

In applications where the readout boards are remotely located, the voltage output of the NCS199AxR can be converted to a precision current output. The precision output current measurements are read more accurately as it overcomes the errors due to ground drops between the boards.

![Figure 35. Surface Mount Kelvin Shunt](image)

As shown in Figure 36, the $R_{\text{OUT}}$ resistor is added between the OUT pin and the REF pin to convert the voltage output to a current output which is taken from the REF pin to the readout board. This circuit is intended to function with low potentials between the boards due to ground drops or noise. The current output is simply the relationship of the normal output voltage of the NCS199AxR:

$$I_{\text{OUT}} = \frac{V_{\text{OUT}}}{R_{\text{OUT}}}$$

A resistor value of 1 kΩ for $R_{\text{OUT}}$ is always a convenient value as it provides 1 mA/V scaling.

On the readout board, for simplicity, $R_{\text{ITOV}}$ can be equal to $R_{\text{OUT}}$ to provide identical voltage drops across both. It is important to take into consideration that $R_{\text{ITOV}}$ and $R_{\text{OUT}}$ add additional voltage drops in the current measurement path. The current source can provide enough compliance to overcome most ground voltage drop, stray voltages, and noise. However, accuracy will degrade if noise or ground drops exceed 1 V.

Shutting Down the NCS199AxR

While the NCS199AxR does not provide a shutdown pin, a simple MOSFET, power switch, or logic gate can be used to switch off the power to the NCS199AxR and eliminate the quiescent current. Note that the shunt input pins will always have a current flow via the input and feedback resistors (total resistance of each leg always equals slightly higher than 1 MΩ). Also note that when powered, the shunt input pins will exhibit the specified and well-matched typical bias current of 39 μA. The shunt input pins support the rated common mode voltage even when the NCS199AxR does not have power applied.
NOTES:
2. CONTROLLING DIMENSION: MILLIMETERS.
3. DIMENSIONS D AND E1 DO NOT INCLUDE MOLD FLASH, PROTRUSIONS, OR GATE BURRS. MOLD FLASH, PROTRUSIONS, OR GATE BURRS SHALL NOT EXCEED 0.20 PER END.
4. DIMENSIONS D AND E1 AT THE OUTERMOST EXTREMES OF THE PLASTIC BODY AND DATUM H.
5. DATUMS A AND B ARE DETERMINED AT DATUM H.
6. DIMENSIONS b AND c APPLY TO THE FLAT SECTION OF THE LEAD BETWEEN 0.08 AND 0.15 FROM THE TIP.
7. DIMENSION b DOES NOT INCLUDE DAMBAR PROTRUSION. ALLOWABLE DAMBAR PROTRUSION SHALL BE 0.08 TOTAL IN EXCESS OF DIMENSION b AT MAXIMUM MATERIAL CONDITION. THE DAMBAR CANNOT BE LOCATED ON THE LOWER RADIUS OF THE FOOT.

**SPECIFIC DEVICE CODE**

**M = Date Code**

**G** or microdot "/C0071" may or may not be present. Some products may not follow the Generic Marking.

**FOR ADDITIONAL INFORMATION ON OUR Pb-FREE STRATEGY AND SOLDERING DETAILS, PLEASE DOWNLOAD THE ON SEMICONDUCTOR SOLDERING AND MOUNTING TECHNIQUES REFERENCE MANUAL, SOLDERRM/D.**

**STYLES ON PAGE 2**
Note: Please refer to datasheet for style callout. If style type is not called out in the datasheet refer to the device datasheet pinout or pin assignment.